General Description

The Micrel MIC26400 is a constant-frequency, synchronous buck regulator featuring a unique digitally modified adaptive ON-time control architecture. The MIC26400 operates over an input supply range of 4.5V to 26V and provides a regulated output at up to 5A of output current. The output voltage is adjustable down to 0.8V with a typical accuracy of ±1%, and the device operates at a switching frequency of 300kHz.

Micrel’s Hyper Speed Control™ architecture allows for ultra-fast transient response while reducing the output capacitance and also makes (High VIN)/(Low VOUT) operation possible. This digitally modified adaptive tON ripple control architecture combines the advantages of fixed frequency operation and fast transient response in a single device.

The MIC26400 offers a full suite of protection features to ensure protection of the IC during fault conditions. These include undervoltage lockout to ensure proper operation under power-sag conditions, internal soft-start to reduce inrush current, foldback current limit, “hiccup” mode short-circuit protection and thermal shutdown.

All support documentation can be found on Micrel’s web site at: www.micrel.com.

Features

- Hyper Speed Control™ architecture enables
  - High delta V operation (VIN = 26V and VOUT = 0.8V)
  - Small output capacitance
- 4.5V to 26V input voltage
- Adjustable output from 0.8V to 5.5V (±1% accuracy)
- Any Capacitor™ Stable
  - Zero ESR to high-ESR output capacitance
- 5A output current capability
- 300kHz switching frequency
- Internal compensation
- Up to 95% efficiency
- 6ms Internal soft-start
- Foldback current limit and “hiccup” mode short-circuit protection
- Thermal shutdown
- Supports safe start-up into a pre-biased load
- −40°C to +125°C junction temperature range
- 28-pin 5mm × 6mm MLF® package

Applications

- Distributed power systems
- Communications/networking infrastructure
- Set-top box, gateways and routers
- Printers, scanners, graphic cards and video cards

Typical Application

Hyper Speed Control, SuperSwitcher II and Any Capacitor are trademarks of Micrel, Inc. MLF and MicroLeadFrame are registered trademarks of Amkor Technology, Inc.
## Ordering Information

<table>
<thead>
<tr>
<th>Part Number</th>
<th>Voltage</th>
<th>Switching Frequency</th>
<th>Junction Temperature Range</th>
<th>Package</th>
<th>Lead Finish</th>
</tr>
</thead>
<tbody>
<tr>
<td>MIC26400YJL</td>
<td>Adjustable</td>
<td>300kHz</td>
<td>−40°C to +125°C</td>
<td>28-Pin 5mm × 6mm MLF®</td>
<td>Pb-Free</td>
</tr>
</tbody>
</table>

## Pin Configuration

![28-Pin 5mm X 6mm MLF® (YJL)](image)

## Pin Description

<table>
<thead>
<tr>
<th>Pin Number</th>
<th>Pin Name</th>
<th>Pin Function</th>
</tr>
</thead>
<tbody>
<tr>
<td>13, 14, 15, 16, 17, 18, 19</td>
<td>PVIN</td>
<td>High-Side N-internal MOSFET Drain Connection (Input): The PVIN operating voltage range is from 4.5V to 26V. Input capacitors between the PVIN pins and the power ground (PGND) are required. Note that the connection must be kept short.</td>
</tr>
<tr>
<td>24</td>
<td>EN</td>
<td>Enable (Input): A logic level control of the output. The EN pin is CMOS-compatible. Logic high or floating = enable, logic low = shutdown. In the off state, the VDD supply current of the device is reduced (typically 0.7mA).</td>
</tr>
<tr>
<td>25</td>
<td>FB</td>
<td>Feedback (Input): Input to the transconductance amplifier of the control loop. The FB pin is regulated to 0.8V. A resistor divider connecting the feedback to the output is used to adjust the desired output voltage.</td>
</tr>
<tr>
<td>26</td>
<td>SGND</td>
<td>Signal ground. SGND must be connected directly to the ground planes. Do not route the SGND pin to the PGND Pad on the top layer. (see PCB Layout Guidelines for details.)</td>
</tr>
<tr>
<td>27</td>
<td>VDD</td>
<td>VDD Bias (Input): Power to the internal reference and control sections of the MIC26400. The VDD operating voltage range is from 4.5V to 5.5V. A 2.2µF ceramic capacitor from the VDD pin-to-PGND must be placed next to the IC.</td>
</tr>
<tr>
<td>2, 5, 6, 7, 8, 21</td>
<td>PGND</td>
<td>Power Ground. PGND is the ground path for the MIC26400 buck converter power stage. The PGND pin connects to the sources of low-side N-Channel internal MOSFETs, the negative terminals of input capacitors, and the negative terminals of output capacitors. The loop for the power ground should be as small as possible and separate from the Signal ground (SGND) loop.</td>
</tr>
<tr>
<td>22</td>
<td>CS</td>
<td>Current Sense (Input): High current output driver return. The CS pin connects directly to the switch node. Due to the high speed switching on this pin, the CS pin should be routed away from sensitive nodes. CS pin also senses the current by monitoring the voltage across the low-side internal MOSFET during OFF-time.</td>
</tr>
<tr>
<td>20</td>
<td>BST</td>
<td>Boost (Output): Bootstrapped voltage to the high-side N-channel internal MOSFET driver. A Schottky diode is connected between the VDD pin and the BST pin. A boost capacitor of 0.1µF is connected between the BST pin and the SW pin.</td>
</tr>
<tr>
<td>4, 9, 10, 11, 12</td>
<td>SW</td>
<td>Switch Node (Output): Internal connection for the high-side MOSFET source and low-side MOSFET drain.</td>
</tr>
<tr>
<td>23</td>
<td>VIN</td>
<td>Power Supply Voltage (Input): Requires bypass capacitor to SGND.</td>
</tr>
<tr>
<td>1, 3, 28</td>
<td>NC</td>
<td>No Connect.</td>
</tr>
</tbody>
</table>

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July 2011
Absolute Maximum Ratings\(^{(1, 2)}\)

- \(PV_{\text{IN}}\) to \(PGND\): \(-0.3\) V to +28 V
- \(V_{\text{IN}}\) to \(PGND\): \(-0.3\) V to \(PV_{\text{IN}}\)
- \(V_{\text{DD}}\) to \(PGND\): \(-0.3\) V to +6 V
- \(V_{\text{SW}}, V_{\text{CS}}\) to \(PGND\): \(-0.3\) V to \((PV_{\text{IN}} + 0.3\) V\)
- \(V_{\text{BST}}\) to \(V_{\text{SW}}\): \(-0.3\) V to 6 V
- \(V_{\text{BST}}\) to \(PGND\): \(-0.3\) V to 34 V
- \(V_{\text{EN}}\) to \(PGND\): \(-0.3\) V to \((V_{\text{DD}} + 0.3\) V\)
- \(V_{\text{FB}}\) to \(PGND\): \(-0.3\) V to \((V_{\text{DD}} + 0.3\) V\)
- PGND to \(SGND\): \(-0.3\) V to +0.3 V
- Junction Temperature: +150°C
- Storage Temperature (TS): −65°C to +150°C
- Lead Temperature (soldering, 10 sec): 260°C

Operating Ratings\(^{(3)}\)

- Supply Voltage (\(PV_{\text{IN}}, V_{\text{IN}}\)): 4.5 V to 26 V
- Output Voltage (\(V_{\text{OUT}}\)): 0.8 V to 5.5 V
- Bias Voltage (\(V_{\text{DD}}\)): 4.5 V to 5.5 V
- Enable Input (\(V_{\text{EN}}\)): 0 V to \(V_{\text{DD}}\)
- Junction Temperature (\(T_J\)): −40°C to +125°C
- Maximum Power Dissipation: Note 4
- Package Thermal Resistance\(^{(4)}\): 5 mm x 6 mm MLF\(^{®}\) (\(\theta_{JA}\)): 36°C/W

Electrical Characteristics\(^{(5)}\)

\(PV_{\text{IN}} = V_{\text{IN}} = 12\) V, \(V_{\text{DD}} = 5\) V; \(V_{\text{BST}} = V_{\text{SW}} = 5\) V; \(T_A = 25°C\), unless noted. Bold values indicate −40°C ≤ \(T_J\) ≤ +125°C.

<table>
<thead>
<tr>
<th>Parameter</th>
<th>Condition</th>
<th>Min.</th>
<th>Typ.</th>
<th>Max.</th>
<th>Units</th>
</tr>
</thead>
<tbody>
<tr>
<td><strong>Power Supply Input</strong></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Input Voltage Range ((V_{\text{IN}}, PV_{\text{IN}}))</td>
<td></td>
<td>4.5</td>
<td>26</td>
<td></td>
<td>V</td>
</tr>
<tr>
<td><strong>(V_{\text{DD}}) Bias Voltage</strong></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Operating Bias Voltage ((V_{\text{DD}}))</td>
<td></td>
<td>4.5</td>
<td>5</td>
<td>5.5</td>
<td>V</td>
</tr>
<tr>
<td>Under-Voltage Lockout Trip Level</td>
<td>(V_{\text{DD}}) Rising</td>
<td>2.4</td>
<td>2.7</td>
<td>3.2</td>
<td>V</td>
</tr>
<tr>
<td>UVLO Hysteresis</td>
<td></td>
<td>50</td>
<td>mV</td>
<td></td>
<td></td>
</tr>
<tr>
<td>Quiescent Supply Current</td>
<td>(V_{\text{FB}} = 1.5) V</td>
<td>1.4</td>
<td>3</td>
<td></td>
<td>mA</td>
</tr>
<tr>
<td>Shutdown Supply Current</td>
<td>(V_{\text{DD}} = V_{\text{BST}} = 5.5) V, (V_{\text{IN}} = 26) V, (SW = ) unconnected, (V_{\text{EN}} = 0) V</td>
<td>0.7</td>
<td>2</td>
<td></td>
<td>mA</td>
</tr>
<tr>
<td><strong>Reference</strong></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Feedback Reference Voltage</td>
<td>(0°C \leq T_J \leq 85°C (\pm 1.0%))</td>
<td>0.792</td>
<td>0.8</td>
<td>0.808</td>
<td>V</td>
</tr>
<tr>
<td></td>
<td>(-40°C \leq T_J \leq 125°C (\pm 1.5%))</td>
<td>0.788</td>
<td>0.8</td>
<td>0.812</td>
<td>V</td>
</tr>
<tr>
<td>Load Regulation</td>
<td>(I_{\text{OUT}} = 0) A to 5 A</td>
<td>0.2</td>
<td></td>
<td></td>
<td>%</td>
</tr>
<tr>
<td>Line Regulation</td>
<td>(V_{\text{IN}} = (V_{\text{OUT}} + 3.0) V) to 26 V</td>
<td>0.1</td>
<td></td>
<td></td>
<td>%</td>
</tr>
<tr>
<td>FB Bias Current</td>
<td>(V_{\text{FB}} = 0.8) V</td>
<td>5</td>
<td></td>
<td></td>
<td>nA</td>
</tr>
<tr>
<td><strong>Enable Control</strong></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>EN Logic Level High</td>
<td>(4.5) V &lt; (V_{\text{DD}} &lt; 5.5) V</td>
<td>1.2</td>
<td>0.85</td>
<td></td>
<td>V</td>
</tr>
<tr>
<td>EN Logic Level Low</td>
<td>(4.5) V &lt; (V_{\text{DD}} &lt; 5.5) V</td>
<td>0.78</td>
<td>0.4</td>
<td></td>
<td>V</td>
</tr>
<tr>
<td>EN Bias Current</td>
<td>(V_{\text{EN}} = 0) V</td>
<td>50</td>
<td></td>
<td></td>
<td>(\mu)A</td>
</tr>
<tr>
<td><strong>Oscillator</strong></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Switching Frequency(^{(6)})</td>
<td></td>
<td>225</td>
<td>300</td>
<td>375</td>
<td>kHz</td>
</tr>
<tr>
<td>Maximum duty cycle(^{(7)})</td>
<td>(V_{\text{FB}} = 0) V</td>
<td>87</td>
<td></td>
<td></td>
<td>%</td>
</tr>
<tr>
<td>Minimum duty cycle</td>
<td>(V_{\text{FB}} &gt; 0.8) V</td>
<td>0</td>
<td></td>
<td></td>
<td>%</td>
</tr>
<tr>
<td>Minimum Off-time(^{(7)})</td>
<td></td>
<td>360</td>
<td></td>
<td></td>
<td>ns</td>
</tr>
<tr>
<td><strong>Soft-Start</strong></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Soft-Start time</td>
<td></td>
<td>6</td>
<td></td>
<td></td>
<td>ms</td>
</tr>
</tbody>
</table>
**Electrical Characteristics** (Continued)

PV\textsubscript{IN} = V\textsubscript{IN} = 12V, V\textsubscript{DD} = 5V; V\textsubscript{BST} – V\textsubscript{SW} = 5V; T\textsubscript{A} = 25°C, unless noted. **Bold** values indicate −40°C ≤ T\textsubscript{J} ≤ +125°C.

<table>
<thead>
<tr>
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<th>Condition</th>
<th>Min.</th>
<th>Typ.</th>
<th>Max.</th>
<th>Units</th>
</tr>
</thead>
<tbody>
<tr>
<td><strong>Short Circuit Protection</strong></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Current-Limit Threshold</td>
<td>V\textsubscript{FB} = 0.8V</td>
<td>6</td>
<td>13</td>
<td></td>
<td>A</td>
</tr>
<tr>
<td>Short Circuit Current</td>
<td>V\textsubscript{FB} = 0V</td>
<td>6</td>
<td></td>
<td></td>
<td>A</td>
</tr>
<tr>
<td><strong>Internal FETs</strong></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Top-MOSFET R\textsubscript{DS (ON)}</td>
<td>I\textsubscript{SW} = 1A</td>
<td>43</td>
<td></td>
<td></td>
<td>mΩ</td>
</tr>
<tr>
<td>Bottom-MOSFET R\textsubscript{DS (ON)}</td>
<td>I\textsubscript{SW} = 1A</td>
<td>12.5</td>
<td></td>
<td></td>
<td>mΩ</td>
</tr>
<tr>
<td>SW Leakage Current</td>
<td>V\textsubscript{IN} = 26V, V\textsubscript{SW} = 26V, V\textsubscript{EN} = 0V, V\textsubscript{BST} = 31.5 V</td>
<td>60</td>
<td></td>
<td></td>
<td>µA</td>
</tr>
<tr>
<td>VIN Leakage Current</td>
<td>V\textsubscript{IN} = 26V, V\textsubscript{SW} = 0V, V\textsubscript{EN} = 0V, V\textsubscript{BST} = 31.5V</td>
<td>25</td>
<td></td>
<td></td>
<td>µA</td>
</tr>
<tr>
<td><strong>Thermal Protection</strong></td>
<td></td>
<td></td>
<td></td>
<td></td>
<td></td>
</tr>
<tr>
<td>Over-temperature Shutdown</td>
<td>T\textsubscript{J} Rising</td>
<td>155</td>
<td></td>
<td></td>
<td>°C</td>
</tr>
<tr>
<td>Hysteresis</td>
<td></td>
<td>10</td>
<td></td>
<td></td>
<td>°C</td>
</tr>
</tbody>
</table>

**Notes:**

1. Exceeding the absolute maximum rating may damage the device.
2. Devices are ESD sensitive. Handling precautions recommended. Human body model, 1.5kΩ in series with 100pF.
3. The device is not guaranteed to function outside operating range.
4. PD\textsubscript{(MAX)} = (T\textsubscript{J\textsubscript{(MAX)}} – T\textsubscript{A})/θ\textsubscript{JA}, where θ\textsubscript{JA} depends upon the printed circuit layout. See “Applications Information.”
5. Specification for packaged product only.
6. Measured in test mode.
7. The maximum duty-cycle is limited by the fixed mandatory off-time t\textsubscript{OFF} of typically 360ns.
Typical Characteristics

Vin Operating Supply Current vs. Input Voltage

Vin Shutdown Current vs. Input Voltage

VDD Operating Supply Current vs. Input Voltage

Feedback Voltage vs. Input Voltage

Total Regulation vs. Input Voltage

Current Limit vs. Input Voltage

Switching Frequency vs. Input Voltage
Typical Characteristics (Continued)

- **V_{DD}** Operating Supply Current vs. Temperature
- **V_{DD}** Shutdown Current vs. Temperature
- **V_{DD}** UVLO Threshold vs. Temperature
- **V_{IN}** Operating Supply Current vs. Temperature
- **V_{IN}** Shutdown Current vs. Temperature
- **V_{IN}** UVLO Threshold vs. Temperature
- **Feedback Voltage vs. Temperature**
- **Load Regulation vs. Temperature**
- **Line Regulation vs. Temperature**
- **Switching Frequency vs. Temperature**
- **EN Bias Current vs. Temperature**

---

**Switching Frequency**

- **V_{IN} = 12V**
- **V_{DD} = 5V**
- **I_{OUT} = 0A**

**EN Bias Current**

- **V_{IN} = 12V**
- **V_{DD} = 5V**

---

**Power Supply Current**

- **SUPPLY CURRENT (mA)**
- **TEMPERATURE (°C)**

- **VIN = 12V**
- **VOUT = 1.2V**
- **VDD = 5V**
- **IOUT = 0A**

---

**Current Limit**

- **CURRENT LIMIT (A)**
- **TEMPERATURE (°C)**

- **VIN = 12V**
- **VDD = 5V**
- **IOUT = 0A**

---

**Load Regulation**

- **LOAD REGULATION (%)**
- **TEMPERATURE (°C)**

- **VIN = 12V**
- **VDD = 5V**
- **IOUT = 0A to 5A**
Typical Characteristics (Continued)
Typical Characteristics (Continued)

Efficiency (VIN = 5V) vs. Output Current

Efficiency (VIN = 12V) vs. Output Current

Efficiency (VIN = 24V) vs. Output Current

Thermal Derating* vs. Ambient Temperature

Die Temperature*: The temperature measurement was taken at the hottest point on the MIC26400 case mounted on a 5 square inch 4 layer, 0.62", FR-4 PCB with 2oz finish copper weight per layer, see Thermal Measurement section. Actual results will depend upon the size of the PCB, ambient temperature and proximity to other heat emitting components.
Functional Characteristics
Functional Characteristics (Continued)
Functional Characteristics (Continued)

Peak Current-Limit Threshold

Output Recovery from Thermal Shutdown

Switching Waveforms $I_{\text{out}} = 5\text{A}$

Switching Waveforms $I_{\text{out}} = 0\text{A}$

Transient Response

$V_{\text{in}} = 12\text{V}$
$V_{\text{out}} = 1.2\text{V}$
$I_{\text{out}} = 13\text{A}$

$V_{\text{in}} = 12\text{V}$
$V_{\text{out}} = 1.2\text{V}$
$I_{\text{out}} = 1.0\text{A}$

$V_{\text{in}} = 12\text{V}$
$V_{\text{out}} = 1.2\text{V}$
$I_{\text{out}} = 5.0\text{A}$

$V_{\text{in}} = 12\text{V}$
$V_{\text{out}} = 1.2\text{V}$
$I_{\text{out}} = 0\text{A}$

$V_{\text{out}} (0.5\text{V/div})$
$I_{\text{out}} (5.0\text{A/div})$

$V_{\text{out}} (0.2\text{V/div})$

Time (40ms/div)
Time (2.0ms/div)

$V_{\text{out}} (5.0\text{V/div})$
$V_{\text{sw}} (5.0\text{V/div})$
$V_{\text{out}} (5.0\text{mV/div})$
$I_{\text{in}} (2.0\text{A/div})$

Time (1.0\mu s/div)
Time (1.0\mu s/div)

$V_{\text{out}} (100\text{mV/div})$
$I_{\text{out}} (5.0\text{A/div})$

Time (200\mu s/div)
Functional Diagram

Figure 1. MIC26400 Block Diagram
Functional Description

The MIC26400 is an adaptive ON-time synchronous step-down DC/DC regulator. It is designed to operate over a wide input voltage range from 4.5V to 26V and provides a regulated output voltage at up to 5A of output current. A digitally modified adaptive ON-time control scheme is employed to obtain a constant switching frequency and to simplify the control compensation. Over-current protection is implemented without the use of an external sense resistor. The device includes an internal soft-start function which reduces the power supply input surge current at start-up by controlling the output voltage rise time.

Theory of Operation

Figure 1 illustrates the block diagram for the control loop of the MIC26400. The output voltage is sensed by the MIC26400 feedback pin FB via the voltage divider R1 and R2, and compared to a 0.8V reference voltage VREF at the error comparator through a low gain transconductance (gm) amplifier. If the feedback voltage decreases and the output of the gm amplifier is below 0.8V, then the error comparator will trigger the control logic and generate an ON-time period. The ON-time period length is predetermined by the "FIXED tON ESTIMATION" circuitry:

\[ t_{ON(estimated)} = \frac{V_{OUT}}{V_{IN} \times 300kHz} \]  

Where \( V_{OUT} \) is the output voltage and \( V_{IN} \) is the power stage input voltage.

At the end of the ON-time period, the internal high-side driver turns off the high-side MOSFET and the low-side driver turns on the low-side MOSFET. The OFF-time period length depends upon the feedback voltage in most cases. When the feedback voltage decreases and the output of the gm amplifier is below 0.8V, the ON-time period will trigger the control logic and generate an OFF-time period. The OFF-time period length is determined by the feedback voltage and the inverting input of the error comparator, which is the same as the feedback voltage.

Figure 2 shows the MIC26400 control loop timing during steady-state operation. During steady-state, the gm amplifier senses the feedback voltage ripple, which is proportional to the output voltage ripple and the inductor current ripple, to trigger the ON-time period. The OFF-time is determined by the gm amplifier. The termination of the OFF-time is controlled by the feedback voltage. At the valley of the feedback voltage ripple, which occurs when \( V_{FB} \) falls below \( V_{REF} \), the OFF period ends and the next ON-time period is triggered through the control logic circuitry.

\[ D_{max} = \frac{t_S - t_{OFF(min)}}{t_S} = 1 - \frac{360ns}{t_S} \]  

where \( t_S = 1/300kHz = 3.33\mu s \).
Figure 3 shows the operation of the MIC26400 during a load transient. The output voltage drops due to the sudden load increase, which causes the $V_{FB}$ to be less than $V_{REF}$. This will cause the error comparator to trigger an ON-time period. At the end of the ON-time period, a minimum OFF-time $t_{OFF(min)}$ is generated to charge $C_{BST}$ since the feedback voltage is still below $V_{REF}$. Then, the next ON-time period is triggered due to the low feedback voltage. Therefore, the switching frequency changes during the load transient, but returns to the nominal fixed frequency once the output has stabilized at the new load current level. With the varying duty cycle and switching frequency, the output recovery time is fast and the output voltage deviation is small in MIC26400 converter.

Unlike true current-mode control, the MIC26400 uses the output voltage ripple to trigger an ON-time period. The output voltage ripple is proportional to the inductor current ripple if the ESR of the output capacitor is large enough. The MIC26400 control loop has the advantage of eliminating the need for slope compensation.

In order to meet the stability requirements, the MIC26400 feedback voltage ripple should be in phase with the inductor current ripple and large enough to be sensed by the $g_m$ amplifier and the error comparator. The recommended feedback voltage ripple is 20mV~100mV. If a low-ESR output capacitor is selected, the feedback voltage ripple may be too small to be sensed by the $g_m$ amplifier and the error comparator. Also, the output voltage ripple and the feedback voltage ripple are not necessarily in phase with the inductor current ripple if the ESR of the output capacitor is very low. In these cases, ripple injection is required to ensure proper operation. Please refer to “Ripple Injection” subsection in “Application Information” for more details about the ripple injection technique.

**Soft-Start**
Soft-start reduces the power supply input surge current at startup by controlling the output voltage rise time. The input surge appears while the output capacitor is charged up. A slower output rise time will draw a lower input surge current.

The MIC26400 implements an internal digital soft-start by making the 0.8V reference voltage $V_{REF}$ ramp from 0 to 100% in about 6ms with 9.7mV steps. Therefore, the output voltage is controlled to increase slowly by a staircase $V_{FB}$ ramp. Once the soft-start cycle ends, the related circuitry is disabled to reduce current consumption. $V_{DD}$ must be powered up at the same time or after $V_{IN}$ to make the soft-start function correctly.

**Current Limit**
The MIC26400 uses the $R_{DS(ON)}$ of the internal low-side power MOSFET to sense over-current conditions. This method will avoid adding cost, board space and power losses taken by a discrete current sense resistor. The low-side MOSFET is used because it displays much lower parasitic oscillations during switching than the high-side MOSFET.

In each switching cycle of the MIC26400 converter, the inductor current is sensed by monitoring the low-side MOSFET in the OFF period. If the inductor current is greater than 13A, then the MIC26400 turns off the high-side MOSFET and a soft-start sequence is triggered. This mode of operation is called “hiccup mode” and its purpose is to protect the downstream load in case of a hard short. The current-limit threshold has a foldback characteristic related to the feedback voltage, as shown in Figure 4.

**Figure 3. MIC26400 Load Transient Response**

**Figure 4. MIC26400 Current Limit Foldback Characteristic**
MOSFET Gate Drive

The Block Diagram of Figure 1 shows a bootstrap circuit, consisting of D1 (a Schottky diode is recommended) and C_{BST}. This circuit supplies energy to the high-side drive circuit. Capacitor C_{BST} is charged, while the low-side MOSFET is on, and the voltage on the SW pin is approximately 0V. When the high-side MOSFET driver is turned on, energy from C_{BST} is used to turn the MOSFET on. As the high-side MOSFET turns on, the voltage on the SW pin increases to approximately V_{IN}. Diode D1 is reversed biased and C_{BST} floats high while continuing to keep the high-side MOSFET on. The bias current of the high-side driver is less than 10mA so a 0.1\mu F to 1\mu F is sufficient to hold the gate voltage with minimal droop for the power stroke (high-side switching) cycle, i.e. \Delta BST = 10mA \times 3.33\mu s/0.1\mu F = 333mV. When the low-side MOSFET is turned back on, C_{BST} is recharged through D1. A small resistor R_G, which is in series with C_{BST}, can be used to slow down the turn-on time of the high-side N-channel MOSFET.

The drive voltage is derived from the V_{DD} supply voltage. The nominal low-side gate drive voltage is V_{DD} and the nominal high-side gate drive voltage is approximately V_{DD} - V_{DIODE}, where V_{DIODE} is the voltage drop across D1. An approximate 30ns delay between the high-side and low-side driver transitions is used to prevent current from simultaneously flowing unimpeded through both MOSFETs.
Application Information

Inductor Selection

Values for inductance, peak, and RMS currents are required to select the output inductor. The input and output voltages and the inductance value determine the peak-to-peak inductor ripple current. Generally, higher inductance values are used with higher input voltages. Larger peak-to-peak ripple currents will increase the power dissipation in the inductor and MOSFETs. Larger output ripple currents will also require more output capacitance to smooth out the larger ripple current. Smaller peak-to-peak ripple currents require a larger inductance value and therefore a larger and more expensive inductor. A good compromise between size, loss and cost is to set the inductor ripple current to be equal to 20% of the maximum output current. The inductance value is calculated by the equation below:

$$L = \frac{V_{OUT} \times (V_{IN(max)} - V_{OUT})}{V_{IN(max)} \times f_{sw} \times 20\% \times I_{OUT(max)}}$$

Where:
- $f_{sw} = $ switching frequency, 300kHz
- $20\% = $ ratio of AC ripple current to DC output current
- $V_{IN(max)} = $ maximum power stage input voltage

The peak-to-peak inductor current ripple is:

$$\Delta I_{L(pp)} = \frac{V_{OUT} \times (V_{IN(max)} - V_{OUT})}{V_{IN(max)} \times f_{sw} \times L}$$

The peak inductor current is equal to the average output current plus one half of the peak-to-peak inductor current ripple:

$$I_{L(pk)} = I_{OUT(max)} + 0.5 \times \Delta I_{L(pp)}$$

The RMS inductor current is used to calculate the $i^2R$ losses in the inductor:

$$I_{L(RMS)} = \sqrt{I_{OUT(max)}^2 + \frac{\Delta I_{L(pp)}^2}{12}}$$

Maximizing efficiency requires the proper selection of core material and minimizing the winding resistance. The high frequency operation of the MIC26400 requires the use of ferrite materials for all but the most cost sensitive applications. Lower cost iron powder cores may be used but the increase in core loss will reduce the efficiency of the power supply. This is especially noticeable at low output power. The winding resistance decreases efficiency at the higher output current levels. The winding resistance must be minimized although this usually comes at the expense of a larger inductor. The power dissipated in the inductor is equal to the sum of the core and copper losses. At higher output loads, the core losses are usually insignificant and can be ignored. At lower output currents, the core losses can be a significant contributor. Core loss information is usually available from the magnetics vendor. Copper loss in the inductor is calculated by the equation below:

$$P_{INDUCTOR(Cu)} = I_{L(RMS)}^2 \times R_{WINDING}$$

The resistance of the copper wire, $R_{WINDING}$, increases with the temperature. The value of the winding resistance used should be at the operating temperature.

$$P_{WINDING(Ht)} = R_{WINDING(20°C)} \times (1 + 0.0042 \times (T_H - T_{20°C}))$$

Where:
- $T_H = $ temperature of wire under full load
- $T_{20°C} = $ ambient temperature
- $R_{WINDING(20°C)} = $ room temperature winding resistance (usually specified by the manufacturer)

Output Capacitor Selection

The type of the output capacitor is usually determined by its ESR (equivalent series resistance). Voltage and RMS current capability are two other important factors for selecting the output capacitor. Recommended capacitor types are tantalum, low-ESR aluminum electrolytic, OSCON and POSCAP. The output capacitor’s ESR is usually the main cause of the output ripple. The output capacitor ESR also affects the control loop from a stability point of view. The maximum value of ESR is calculated:

$$ESR_{C_{OUT}} \leq \frac{\Delta V_{OUT(pp)}}{\Delta I_{L(pp)}}$$

where:
- $\Delta V_{OUT(pp)} = $ peak-to-peak output voltage ripple
- $\Delta I_{L(pp)} = $ peak-to-peak inductor current ripple
The total output ripple is a combination of the ESR and output capacitance. The total ripple is calculated below:

$$\Delta V_{OUT(pp)} = \sqrt{\left(\frac{\Delta I_{L(pp)}}{C_{OUT} \times f_{SW} \times 8}\right)^2 + \left(\frac{\Delta I_{L(pp)} \times ESR_{OUT}}{2}\right)^2}$$

(11)

Where:
- \(D\) = duty cycle
- \(C_{OUT}\) = output capacitance value
- \(f_{SW}\) = switching frequency

As described in the "Theory of Operation" subsection in "Functional Description", the MIC26400 requires at least 20mV peak-to-peak ripple at the FB pin to make the \(g_m\) amplifier and the error comparator behave properly. Also, the output voltage ripple should be in phase with the inductor current. Therefore, the output voltage ripple caused by the output capacitors value should be much smaller than the ripple caused by the output capacitor ESR. If low-ESR capacitors, such as ceramic capacitors, are selected as the output capacitors, a ripple injection method should be applied to provide the enough feedback voltage ripple. Please refer to the "Ripple Injection" subsection for more details.

The voltage rating of the capacitor should be twice the output voltage for a tantalum and 20% greater for aluminum electrolytic or OS-CON. The output capacitor RMS current is calculated below:

$$I_{C_{OUT}(RMS)} = \frac{\Delta I_{L(pp)}}{\sqrt{12}}$$

(12)

The power dissipated in the output capacitor is:

$$P_{DISS(C_{OUT})} = I_{C_{OUT}(RMS)}^2 \times ESR_{C_{OUT}}$$

(13)

### Input Capacitor Selection

The input capacitor for the power stage input \(V_{IN}\) should be selected for ripple current rating and voltage rating. Tantalum input capacitors may fail when subjected to high inrush currents, caused by turning the input supply on. A tantalum input capacitor's voltage rating should be at least two times the maximum input voltage to maximize reliability. Aluminum electrolytic, OS-CON, and multilayer polymer film capacitors can handle the higher inrush currents without voltage de-rating. The input voltage ripple will primarily depend on the input capacitor's ESR.

The peak input current is equal to the peak inductor current, so:

$$\Delta V_{IN} = I_{L(pk)} \times ESR_{C_{IN}}$$

(14)

The input capacitor must be rated for the input current ripple. The RMS value of input capacitor current is determined at the maximum output current. Assuming the peak-to-peak inductor current ripple is low:

$$I_{C_{IN}(RMS)} \approx I_{OUT(max)} \times \sqrt{D \times (1-D)}$$

(15)

The power dissipated in the input capacitor is:

$$P_{DISS(C_{IN})} = I_{C_{IN}(RMS)}^2 \times ESR_{C_{IN}}$$

(16)

### Ripple Injection

The \(V_{FB}\) ripple required for proper operation of the MIC26400 \(g_m\) amplifier and error comparator is 20mV to 100mV. However, the output voltage ripple is generally designed as 1% to 2% of the output voltage. For a low output voltage, such as a 1V, the output voltage ripple is only 10mV to 20mV, and the feedback voltage ripple is less than 20mV. If the feedback voltage ripple is so small that the \(g_m\) amplifier and error comparator can’t sense it, the MIC26400 will lose control and the output voltage is not regulated. In order to have some amount of \(V_{FB}\) ripple, a ripple injection method is applied for low output voltage ripple applications.

The applications are divided into three situations according to the amount of the feedback voltage ripple:

1) Enough ripple at the feedback voltage due to the large ESR of the output capacitors.

As shown in Figure 5a, the converter is stable without any ripple injection. The feedback voltage ripple is:

$$\Delta V_{FB(pp)} = \frac{R2}{R1 + R2} \times ESR_{C_{OUT}} \times \Delta I_{L(pp)}$$

(17)

where \(\Delta I_{L(pp)}\) is the peak-to-peak value of the inductor current ripple.

2) Inadequate ripple at the feedback voltage due to the small ESR of the output capacitors.

The output voltage ripple is fed into the FB pin through a feedforward capacitor \(C_f\) in this situation, as shown in Figure 5b. The typical \(C_f\) value is between 1nF and 100nF.
With the feedforward capacitor, the feedback voltage ripple is very close to the output voltage ripple:

\[ \Delta V_{FB(pp)} \approx \text{ESR} \times \Delta I_{L(pp)} \]  

(18)

3) Virtually no ripple at the FB pin voltage due to the very low ESR of the output capacitors.

In this situation, the output voltage ripple is less than 20mV. Therefore, additional ripple is injected into the FB pin from the switching node SW via a resistor \( R_{inj} \) and a capacitor \( C_{inj} \), as shown in Figure 5c. The injected ripple is:

\[ \Delta V_{FB(pp)} = V_{IN} \times K_{\text{div}} \times D \times (1-D) \times \frac{1}{f_{SW} \times \tau} \]  

(19)

\[ K_{\text{div}} = \frac{R_{1//R2}}{R_{inj} + R_{1//R2}} \]  

(20)

Where:

- \( V_{IN} \) = Power stage input voltage
- \( D \) = duty cycle
- \( f_{SW} \) = switching frequency
- \( \tau = (R_{1//R2//R_{inj}}) \times C_{ff} \)

In equations (19) and (20), it is assumed that the time constant associated with \( C_{ff} \) must be much greater than the switching period:

\[ \frac{1}{f_{SW} \times \tau} = \frac{T}{\tau} \ll 1 \]  

(21)

If the voltage divider resistors \( R1 \) and \( R2 \) are in the kΩ range, a \( C_{ff} \) of 1nF to 100nF can easily satisfy the large time constant requirements. Also, a 100nF injection capacitor \( C_{inj} \) is used in order to be considered as short for a wide range of the frequencies.

The process of sizing the ripple injection resistor and capacitors is:

**Step 1.** Select \( C_{ff} \) to feed all output ripples into the feedback pin and make sure the large time constant assumption is satisfied. Typical choice of \( C_{ff} \) is 1nF to 100nF if \( R1 \) and \( R2 \) are in kΩ range.

**Step 2.** Select \( R_{inj} \) according to the expected feedback voltage ripple using equation (22),

\[ K_{\text{div}} = \frac{\Delta V_{FB(pp)}}{V_{IN}} \times \frac{f_{SW} \times \tau}{D \times (1-D)} \]  

(22)
Then the value of $R_{\text{inj}}$ is obtained as:

$$R_{\text{inj}} = (R1//R2) \times \left( \frac{1}{K_{\text{div}}} - 1 \right) \quad (23)$$

**Step 3.** Select $C_{\text{inj}}$ as 100nF, which could be considered as short for a wide range of the frequencies.

**Setting Output Voltage**

The MIC26400 requires two resistors to set the output voltage as shown in Figure 6.

![Figure 6. Voltage-Divider Configuration](image)

The output voltage is determined by the equation:

$$V_{\text{OUT}} = V_{\text{FB}} \times \left( 1 + \frac{R1}{R2} \right) \quad (24)$$

Where $V_{\text{FB}} = 0.8V$. A typical value of $R1$ can be between 3kΩ and 10kΩ. If $R1$ is too large, it may allow noise to be introduced into the voltage feedback loop. If $R1$ is too small in value, it will decrease the efficiency of the power supply, especially at light loads. Once $R1$ is selected, $R2$ can be calculated using:

$$R2 = \frac{V_{\text{FB}} \times R1}{V_{\text{OUT}} - V_{\text{FB}}} \quad (25)$$

In addition to the external ripple injection added at the FB pin, internal ripple injection is added at the inverting input of the comparator inside the MIC26400, as shown in Figure 7. The inverting input voltage $V_{\text{INJ}}$ is clamped to 1.2V. As $V_{\text{OUT}}$ is increased, the swing of $V_{\text{INJ}}$ will be clamped. The clamped $V_{\text{INJ}}$ reduces the line regulation because it is reflected back as a DC error on the FB terminal. Therefore, the maximum output voltage of the MIC26400 should be limited to 5.5V to avoid this line regulation problem.

**Thermal Measurements**

Measuring the IC’s case temperature is recommended to insure it is within its operating limits. Although this might seem like a very elementary task, it is easy to get erroneous results. The most common mistake is to use the standard thermal couple that comes with a thermal meter. This thermal couple wire gauge is large, typically 22 gauge, and behaves like a heatsink, resulting in a lower case measurement.

Two methods of temperature measurement are using a smaller thermal couple wire or an infrared thermometer. If a thermal couple wire is used, it must be constructed of 36 gauge wire or higher (smaller wire size) to minimize the wire heat-sinking effect. In addition, the thermal couple tip must be covered in either thermal grease or thermal glue to make sure that the thermal couple junction is making good contact with the case of the IC. Omega brand thermal couple (5SC-TT-K-36-36) is adequate for most applications.

Wherever possible, an infrared thermometer is recommended. The measurement spot size of most infrared thermometers is too large for an accurate reading on a small form factor ICs. However, a IR thermometer from Optris has a 1mm spot size, which makes it a good choice for measuring the hottest point on the case. An optional stand makes it easy to hold the beam on the IC for long periods of time.
PCB Layout Guidelines

Warning!!! To minimize EMI and output noise, follow these layout recommendations.

PCB Layout is critical to achieve reliable, stable and efficient performance. A ground plane is required to control EMI and minimize the inductance in power, signal and return paths.

The following guidelines should be followed to insure proper operation of the MIC26400 converter.

IC

- The 2.2µF ceramic capacitor, which is connected to the VDD pin, must be located right at the IC. The VDD pin is very noise sensitive and placement of the capacitor is very critical. Use wide traces to connect to the VDD and PGND pins.
- The signal ground pin (SGND) must be connected directly to the ground planes. Do not route the SGND pin to the PGND Pad on the top layer.
- Place the IC close to the point of load (POL).
- Use fat traces to route the input and output power lines.
- Signal and power grounds should be kept separate and connected at only one location.

Input Capacitor

- Place the input capacitor next.
- Place the input capacitors on the same side of the board and as close to the IC as possible.
- Keep both the PVIN and PGND connections short.
- Place several vias to the ground plane close to the input capacitor ground terminal.
- Use either X7R or X5R dielectric input capacitors. Do not use Y5V or Z5U type capacitors.
- Do not replace the ceramic input capacitor with any other type of capacitor. Any type of capacitor can be placed in parallel with the input capacitor.
- If a Tantalum input capacitor is placed in parallel with the input capacitor, it must be recommended for switching regulator applications and the operating voltage must be derated by 50%.
- In “Hot-Plug” applications, a Tantalum or Electrolytic bypass capacitor must be used to limit the over-voltage spike seen on the input supply with power is suddenly applied.

Inductor

- Keep the inductor connection to the switch node (SW) short.
- Do not route any digital lines underneath or close to the inductor.
- Keep the switch node (SW) away from the feedback (FB) pin.
- The CS pin should be connected directly to the SW pin to accurate sense the voltage across the low-side MOSFET.
- To minimize noise, place a ground plane underneath the inductor.

Output Capacitor

- Use a wide trace to connect the output capacitor ground terminal to the input capacitor ground terminal.
- Phase margin will change as the output capacitor value and ESR changes. Contact the factory if the output capacitor is different from what is shown in the BOM.
- The feedback trace should be separate from the power trace and connected as close as possible to the output capacitor. Sensing a long high current load trace can degrade the DC load regulation.

RC Snubber

- Place the RC snubber on the same side of the board and as close to the SW pin as possible.
Figure 8. Schematic of MIC26400 Evaluation Board

(J13, R13, R15 are for testing purposes)
## Bill of Materials

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### Notes:
1. EPCOS: [www.epcos.com](http://www.epcos.com).
2. AVX: [www.avx.com](http://www.avx.com).
4. TDK: [www.tdk.com](http://www.tdk.com).
5. SANYO: [www.sanyo.com](http://www.sanyo.com).
7. Vishay: [www.vishay.com](http://www.vishay.com).
PCB Layout

Figure 9. MIC26400 Evaluation Board Top Layer

Figure 10. MIC26400 Evaluation Board Mid-Layer 1 (Ground Plane)
PCB Layout (Continued)

Figure 11. MIC26400 Evaluation Board Mid-Layer 2

Figure 12. MIC26400 Evaluation Board Bottom Layer
Recommended Land Pattern
Package Information

**TOP VIEW**

**BOTTOM VIEW**

**SIDE VIEW**

28-Lead 5mm x 6mm MLF® (YJL)

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